

MULTIPLIER-DIVIDER CIRCUIT FOR A PFC CONTROLLER

BACKGROUND OF THE INVENTION

Field of the Invention

[0001] The present invention relates to the art of power supplies, and in particular to an analog multiplier-divider for a power factor correction (PFC) circuit.

Description of the Prior Art

[0002] There are many uses for analog multiplier-dividers in modern electronics. Multiplier-dividers produce an output signal that is proportional to a ratio of two or more input signals. The input and output signals can either be voltages or currents.

[0003] One common use of multiplier-dividers is in power factor correction (PFC) circuits. PFC circuits commonly use multiplier-dividers to generate a control signal based on the input current, the feedback signal, and the input voltage. FIG. 1 demonstrates the use of an analog multiplier-divider in a PFC circuit.

[0004] There are many known ways of constructing analog multiplier-dividers, such as logarithmic amplifiers and antilog amplifiers. The implementation of a logarithmic amplifier normally uses the p-n junction volt-ampere characteristic; it is given by

$$I_D = I_0 \times [\exp(V_D / \eta V_T) - 1] \text{ ----- (1)}$$

where I_0 is the reverse saturation current; V_D is the forward bias voltage; η is the constant; $V_T = T / 11,600$ and T is the temperature °K. Since the output current I_D is the exponential function of the forward bias voltage V_D , the linear operating region is small.

The book "Analog Integrated Circuit Design" by David A. Johns and Ken Martin (1997, pg. 366-367) teaches a known analog multiplier-divider. This particular multiplier-divider is also referred to as a four-quadrant multiplier. It is shown in FIG. 2.

[0005] The prior-art analog multiplier-divider shown in FIG. 2 supplies an output current with an amplitude that is proportional to the product of a first input current and a current ratio. The current ratio is equal to the amplitude of a second input current divided by the amplitude of a bias current. The prior-art multiplier-divider shown in FIG. 2 is built using bipolar transistor devices.

[0006] Many other known prior-art multiplier-dividers exist that are based on the principles of the prior-art multiplier-divider shown in FIG. 2. They all share the same disadvantages, to the extent that they are built using bipolar transistor devices.

[0007] One disadvantage of the prior-art multiplier-divider shown in FIG. 2 is that it is a bipolar device. For many present-day applications, such as PFC circuits, integrated circuits manufactured using a bipolar process are not suitable, because their die-size is too large and the cost is too high.

[0008] Another disadvantage of the prior-art multiplier-divider shown in FIG. 2 is that the output of the circuit varies significantly with temperature. The characteristic equations of bipolar transistors have high temperature coefficients. Thus, the output of the circuit is highly susceptible to temperature changes.

[0009] Another disadvantage of the prior-art multiplier-divider shown in FIG. 2 is high power consumption. The prior-art multiplier-divider requires a constant non-zero biasing current to bias bipolar transistors in linear mode. This results in significant power consumption.

[0010] Another disadvantage of the prior-art multiplier-divider shown in FIG. 2

is poor noise immunity. The prior-art multiplier-divider uses high-gain bipolar transistor devices. With such devices, even relatively small input signal distortion can result in significant output signal distortion.

[0011] Another disadvantage of the prior-art multiplier-divider shown in FIG. 2 is that it has a narrow input range, limited to the linear operating region of bipolar transistors. Outside of this narrow input signal range, the multiplier-divider shown in FIG. 2 is highly susceptible to distortion.

[0012] Therefore, there is a need for an improved analog multiplier-divider. In particular, there is a need for an improved analog multiplier-divider that has a smaller die size while being suitable for a wider range of operating temperatures.

SUMMARY OF THE INVENTION

[0013] The multiplier-divider according to the present invention produces an output signal in response to a first multiplier-signal, a second multiplier-signal and a divisor-signal. The output signal is proportional to the product of the first multiplier-input signal and the second multiplier-input signal divided by the square of the divisor-input signal.

[0014] The multiplier-divider according to the present invention itself consists of two multiplier-divider stages cascaded together. A pulse generator is used to regulate the operation of the cascaded multiplier-divider stages. Each multiplier-divider stage consists of a charge-time control circuit, a linear charging block, and a sample-and-hold circuit.

[0015] The charge-time control circuit of each multiplier-divider stage produces a charge-time for the linear charging block. To perform division, the charge-time is

modulated by a sawtooth signal, with a peak value proportional to the divisor-input signal. The length of the charge-time and the magnitude of the charge current are respectively determined in response to the first multiplier-signal and the second multiplier-signal of the multiplier-divider. The linear charging block of each multiplier-divider stage will be charged so that when sampled, it will output a voltage signal proportional to an appropriate ratio of the input signals.

[0016] Briefly, the multiplier-divider according to the present invention is built according to the principles of capacitor charge theory. The voltage across the capacitor is proportional to the product of the charge current and the charge time interval, and is divided by the capacitance of the capacitor. By using a modulated charge current and a programmable charge time to switch the capacitor, the voltage across the capacitor can be controlled. This capacitor voltage is also the output voltage of the multiplier-divider.

[0017] A general objective of the present invention is to provide an analog multiplier-divider for a power factor correction circuit of a switch-mode power supply. The multiplier-divider according to the present invention is intended for low speed applications that generally operate at internal clock rates of less than 100kHz.

[0018] Another objective of the present invention is to provide an analog multiplier-divider that is manufactured using CMOS fabrication. The multiplier-divider according to the present invention exclusively uses MOSFET-based devices. Therefore, the multiplier-divider according to the present invention can be manufactured at a significantly reduced die-size, and at a lower cost, than the prior-art multiplier-dividers.

[0019] Another objective of the present invention is to provide an analog multiplier-divider having a characteristic equation that is substantially temperature-independent, compared to the prior-art multiplier-divider. The multiplier-divider

according to the present invention is constructed from MOSFET-devices. Thus, the temperature coefficient of the multiplier-divider according to the present invention is low. The multiplier-divider according to the present invention can operate successfully over a very wide temperature range.

[0020] Another objective of the present invention is to provide an analog multiplier-divider with reduced power consumption. The multiplier-divider according to the present invention does not require a constant biasing current.

[0021] Another objective of the present invention is to provide an analog multiplier-divider with improved noise immunity. The accuracy of the output signal of the multiplier-divider according to the present invention is not significantly affected by small noise components from the input signals.

[0022] Still further objects and advantages will become apparent from a consideration of the ensuing description and drawings.

BRIEF DESCRIPTION OF THE DRAWINGS

[0023] The accompanying drawings are included to provide a further understanding of the invention, and are incorporated in and constitute a part of this specification. The drawings illustrate embodiments of the invention and, together with the description, serve to explain the principles of the invention.

[0024] FIG. 1 shows a schematic diagram of a switch mode power supply with a power factor correction circuit including a multiplier-divider.

[0025] FIG. 2 shows a block diagram of a prior-art multiplier-divider.

[0026] FIG. 3 shows a block diagram of a multiplier-divider according to the present invention.

[0027] FIG. 4 shows a pulse generator of the multiplier-divider according to the present invention.

[0028] FIG. 5 shows a detailed block diagram of a sawtooth signal generator of the pulse generator according to the present invention.

[0029] FIG. 6 shows a detailed block diagram of a variable current sink of the sawtooth-signal generator according to the present invention.

[0030] FIG. 7 shows a detailed block diagram of a first multiplier-divider stage of the multiplier-divider according to the present invention.

[0031] FIG. 8 shows a detailed block diagram of a second multiplier-divider stage of the multiplier-divider according to the present invention.

according to the present invention; and

[0032] FIG. 9 shows a timing diagram of the pulse generator according to the present invention.

DESCRIPTION OF THE PREFERRED EMBODIMENTS

[0033] Referring now to the drawings wherein the contents are for purposes of illustrating the preferred embodiment of the invention only and not for purposes of limiting same, FIG. 2 shows a prior-art multiplier-divider.

[0034] The prior-art multiplier-divider is constructed from an array of six bipolar transistors. The multiplier-divider includes six transistors 10, 11, 12, 13, 14 and 15. A base of each of the transistors 10, 11, 12, 13, 14 and 15 are tied together.

[0035] A collector of the transistor 10 is connected to the base of the transistor 10. An emitter of the transistor 10 is connected to the ground reference. The collector of the transistor 10 is connected to a first positive input terminal I_1 . A collector of the

transistor 11 is connected to a negative output terminal I'_O . A collector of the transistor 12 is connected to a positive output terminal I_O . A collector of the transistor 13 is connected to the negative output terminal I'_O . An emitter of the transistor 12 and an emitter of the transistor 13 are connected to a second positive input terminal I_2 . A collector of the transistor 14 is connected to the positive output terminal I_O . An emitter of the transistor 11 and an emitter of the transistor 14 are connected to a second negative input terminal I'_2 . A collector of the transistor 15 is connected to a first negative input terminal I'_1 . The collector of the transistor 15 is connected to the base of the transistor 15. An emitter of the transistor 15 is connected to the ground reference. Operation of this circuit will be well known to those skilled in the art and therefore detailed description thereof is omitted herein.

[0036] As discussed above, one major drawback of this prior-art multiplier-divider is that it is constructed using bipolar devices. This results in a large die-size, and introduces a high degree of temperature dependence into the characteristic of the multiplier-divider. For these reasons, the prior-art multiplier-divider shown in FIG. 2 is not suitable for use in a power converter with power factor correction (PFC). FIG. 1 shows such a power converter. The power converter having power factor correction comprises an AC-power source 50, a rectifier 51, an inductor 52, a diode 53, two capacitors 54 and 61, a switch 55, four resistors 56, 57 58 and 60, two comparators 59 and 62, a gate-driver 63 and a PFC circuit. The PFC circuit of FIG. 1 includes six resistors 64, 65, 67, 101, 102 and 103, a comparator 66, two capacitors 68 and 104, and a V-to-I converter 69. The PFC circuit further includes a multiplier-divider 100.

[0037] The power converter shown in FIG. 1 is a standard power supply known in the art. An input of the power supply is the AC-power source 50. The AC-power

source **50** is coupled to a first input and to a second input of the rectifier **51**. A first output of the rectifier **51** is connected to a first terminal of the inductor **52**. A second terminal of the inductor **52** is connected to an anode of a diode **53**. A cathode of the diode **53** is connected to an output voltage terminal V_{OUT} . The capacitor **54** is connected between the output voltage terminal V_{OUT} and the ground reference. The switch **55** is connected between the second terminal of the inductor **52** and the ground reference.

[0038] To provide a feedback signal to the PFC circuit, the output voltage terminal V_{OUT} is also connected to the ground reference via a resistor-divider network. The resistor-divider network consists of two resistors **64** and **65** connected in series. A junction of the resistor **64** and the resistor **65** is connected to a negative input of the comparator **66**. A positive input of the comparator **66** is supplied with a reference voltage V_R . The negative input of the comparator **66** is connected to an output of the comparator **66** via a resistor **67** and a capacitor **68**.

[0039] The output of the comparator **66** supplies a first multiplier-signal V_E to a first multiplier-input terminal **VE** of the multiplier-divider **100**. A divisor-input terminal **VAC** of the multiplier-divider **100** is supplied with a divisor-signal V_{AC} . The divisor-input terminal **VAC** of the multiplier-divider **100** is also connected to the ground reference via the resistor **103**. The capacitor **104** is connected in parallel with the resistor **103**. An input voltage V_{IN} is supplied to the divisor-input terminal **VAC** via the resistor **103**. An input voltage V_{IN} is supplied to the divisor-input terminal **VAC** via the resistor **102**. A second multiplier-input terminal **IAC** of the multiplier-divider **100** is supplied with the input voltage V_{IN} via the resistor **101**. The resistor **101** transfers the input voltage V_{IN} into a second multiplier-signal I_{AC} . An output terminal **OUT** of the multiplier-divider **100** supplies an output signal V_O to an input of the V-to-I converter **69**.

[0040] An output of the V-to-I converter 69 generates a voltage V_M . The voltage V_M is supplied to a second output of the rectifier 51 via the resistor 57. A positive input of the comparator 59 is also supplied with the voltage V_M . A negative input of the comparator 59 is connected to the ground reference via the resistor 58. The negative input of the comparator 59 is also connected to an output of the comparator 59, via the resistor 60 and the capacitor 61. The resistor 56 is connected between the second output of the rectifier 51 and the ground reference. The output of the comparator 59 is connected to a positive input of the comparator 62. A negative input of the comparator 62 is supplied with a sawtooth-signal V_{SAW} . An output of the comparator 62 drives the switch 55 via the gate-driver 63. The operation of this circuit will be well known to those skilled in the art and therefore detailed description thereof will be omitted herein.

[0041] To overcome the problems of the prior-art multiplier-divider, the present invention proposes an analog multiplier-divider constructed from MOSFET devices. FIG. 3 shows a block diagram of the multiplier-divider 100 according to the present invention. The multiplier-divider 100 has a first multiplier-input terminal **VE** for receiving a first multiplier-signal V_E , a second multiplier-input terminal **IAC** for receiving a second multiplier-signal I_{AC} , and a divisor-input terminal **VAC** for receiving a divisor-signal V_{AC} . The multiplier-divider 100 also has an output terminal **OUT**, which provides an output signal V_O . The magnitude of the output signal V_O is proportional to the magnitude of the first multiplier-signal V_E multiplied by the magnitude of the second multiplier-signal I_{AC} , divided by the square of the magnitude of the divisor-signal V_{AC} . The output signal V_O of the multiplier-divider 100 can be expressed as,

$$V_O \propto I_R \times \left(\frac{I_{AC} \times V_E}{V_{AC}^2} \right) \text{-----} (2)$$

where the current I_R is constant.

[0042] According to the present invention, the second multiplier-signal I_{AC} and the constant current I_R are current signals while the first multiplier-signal V_E , the divisor-signal V_{AC} and the output signal V_O are voltage signals.

[0043] The multiplier-divider 100 consists of a first multiplier-divider stage 130, a second multiplier-divider stage 150, and a pulse generator 200. The first multiplier-divider stage 130 and the second multiplier-divider stage 150 are both multiplier-dividers. Each multiplier-divider has three inputs and an output. In the multiplier-divider 100, the first multiplier-divider stage 130 and the second multiplier-divider stage 150 are cascaded to obtain the desired output signal V_O .

[0044] The pulse generator 200 generates signals including a pulse-signal PLS , an inversed pulse-signal $/PLS$, a clear-signal CLR , a sawtooth-signal V_{SAW} , and a sample-signal SMP . Above signals are respectively supplied to the first multiplier-divider stage 130 and the second multiplier-divider stage 150 to control the operation of the multiplier-divider 100.

[0045] The first multiplier-divider stage 130 has a first input connected to the first multiplier-input VE of the multiplier-divider 100. The first multiplier-divider stage 130 further has a second input driven by a constant current source 135, which provides a constant current I_R . The first multiplier-divider stage 130 further has a third input connected to the divisor-input terminal VAC of the multiplier-divider 100.

[0046] The second multiplier-divider stage 150 has a first input supplied with an output signal V_1 of the first multiplier-divider stage 130. The second multiplier-divider stage 150 further has a second input connected to the second multiplier-input terminal

IAC of the multiplier-divider **100**. The second multiplier-divider stage **150** further has a third input connected to the divisor-input terminal **VAC** of the multiplier-divider **100**.

[0047] FIG. 4 shows the pulse generator **200**. The pulse generator **200** includes a sawtooth-signal generator **110**, a current source **210**, a switch **211**, a switch **212**, and a current sink **213**. The pulse generator **200** further includes a capacitor **220**, a hysteresis comparator **221** and two NOT-gates **222** and **223**. The pulse generator **200** further includes a comparator **230**, three NOT-gates **231** **232** and **242**, and two NAND-gates **240** and **241**. The pulse generator **200** further includes three NOT-gates **250**, **251** and **252**, and an AND-gate **253**. The pulse generator **200** further includes four NOT-gates **260**, **261**, **262** and **271**, an AND-gate **263** and a NAND-gate **270**.

[0048] An input of the current source **210** is connected to a voltage source V_{DD} . The switch **211** is connected between an output of the current source **210** and an input junction. The switch **212** is connected between the input junction and an input of the current sink **213**. An output of the current sink **213** is connected to the ground reference. An input of the hysteresis comparator **221** is connected to the input junction. The capacitor **220** is connected between the input of the hysteresis comparator **221** and the ground reference. An output of the hysteresis comparator **221** is connected to an input of the NOT-gate **222**. An output of the NOT-gate **222** is connected to an input of the NOT-gate **223**. An output of the NOT-gate **223** provides a signal V_R .

[0049] A positive input of the comparator **230** is connected to an output terminal of the sawtooth signal generator **110**. A negative input of the comparator **230** is supplied with a reference voltage V_{REF} . An output of the comparator **230** is connected to an input of the NOT-gate **231**. An output of the NOT-gate **231** is connected to an input of the NOT-gate **232**. An output of the NOT-gate **232** provides a signal V_S .

[0050] A first input of the NAND-gate 240 is driven by the signal V_R . A second input of the NAND-gate 240 is connected to an output of the NOT-gate 241. A first input of the NAND-gate 241 is connected to an output of the NAND-gate 240. A second input of the NAND-gate 241 is driven by the signal V_S . The output of the NAND-gate 240 supplies a signal CK_1 to drive a control terminal of the switch 211 via the NOT-gate 242. Further, a control terminal of the switch 212 is also supplied with the signal CK_1 .

[0051] An input of the NOT-gate 250 is driven by the signal CK_1 . An input of the NOT-gate 251 is connected to an output of the NOT-gate 250. An input of the NOT-gate 252 is connected to an output of the NOT-gate 251. An output of the NOT-gate 252 is connected to an input of the AND-gate 253. An inverted input of the AND-gate 253 is supplied with the signal CK_1 . An output of the AND-gate 253 supplies the sample-signal **SMP** of the pulse generator 200. An input of the NOT-gate 260 is supplied with the signal V_R . An input of the NOT-gate 261 is connected to an output of the NOT-gate 260. An input of the NOT-gate 262 is connected to an output of the NOT-gate 261. An output of the NOT-gate 262 is connected to an input of the AND-gate 263. An inverted input of the AND-gate 263 is supplied with the signal V_R . An output of the AND-gate 263 supplies the clear-signal **CLR**.

[0052] A first input of the NAND-gate 270 is supplied with the signal CK_1 . A second input of the NAND-gate 270 is supplied with the signal V_R . An output of the NAND-gate 270 supplies the pulse-signal **PLS** and supplies the inversed pulse-signal **/PLS** via the NOT-gate 271. The operation of the pulse generator 200 will be well known to those skilled in the art and therefore is discussed detail herein.

[0053] FIG. 5 shows the sawtooth-signal generator 110 according to a preferred embodiment of the present invention. The sawtooth signal generator 110 comprises a switch 111, a switch 112, a capacitor 113, and a variable current sink 120. A control terminal of the switch 111 is supplied with the pulse-signal PLS. A control terminal of the switch 112 is supplied with the inversed pulse-signal /PLS. An input terminal of the switch 111 is connected to the divisor-input terminal VAC. An output terminal of the switch 111 is connected to an input terminal of the switch 112. The capacitor 113, generates the sawtooth signal V_{SAW} , is connected between the output terminal of the switch 111 and the ground reference. An output terminal of the switch 112 is connected to the ground reference via the variable current sink 120. A control terminal of the variable current sink 120 is connected to the divisor-input terminal VAC.

[0054] When the pulse generator 200 supplies a logic-high pulse-signal PLS, the switch 111 will close. This will cause the capacitor 113 to be promptly charged to a voltage level of the divisor-signal V_{AC} . When the pulse-signal PLS goes low, the switch 112 will close, and the switch 111 will open. At this point, the capacitor 113 will begin to discharge. The variable current sink 120 will discharge the capacitor 113. To ensure that the discharge time will be independent of the divisor-input signal V_{AC} , the dynamic current sink 120 generates a sink current I_1 that is proportional to the magnitude of the divisor-input signal V_{AC} .

[0055] FIG. 6 shows the variable current sink 120 according to a preferred embodiment of the present invention. The variable current sink 120 generates the sink current I_1 that is proportional to the magnitude of the divisor-input signal V_{AC} . This property is used to regulate the discharge time of the capacitor 113, so that the length of

the sawtooth period will be independent of the magnitude of the divisor-signal of the multiplier-divider 100.

[0056] The variable current sink 120 comprises an operation amplifier 121, a resistor 122, and a MOSFET 123. A positive terminal of the operation amplifier 121 is connected to the control terminal of the variable current sink 120. A negative terminal of the amplifier 121 is connected to a source of the MOSFET 123. The source of the MOSFET 123 is connected to an output terminal of the variable current sink 120 via the resistor 122. An output terminal of the operation amplifier 121 is connected to a gate of the MOSFET 123. A drain of the MOSFET 123 is connected to an input terminal of the variable current sink 120. The variable current sink 120 will sink the sink current I_1 that is proportional to the magnitude of the divisor-input signal V_{AC} , divided by the resistance of the resistor 122. Operation of this circuit will be well known to those skilled in the art and therefore a detailed description thereof is omitted herein.

[0057] FIG. 7 shows the first multiplier-divider stage 130 of the multiplier-divider 100 according to a preferred embodiment of the present invention. The first multiplier-divider stage 130 comprises of a charge-time control circuit, a linear charging block, and a sample-and-hold circuit.

[0058] The charge-time control circuit of the first multiplier-divider stage 130 includes a comparator 131 and an AND-gate 132. A negative input of the comparator 131 is supplied with the sawtooth signal V_{SAW} . A positive input of the comparator 131 is connected to the first multiplier-input terminal VE . An output of the comparator 131 is connected to a first input of the AND-gate 132. A second input of the AND-gate 132 is supplied with the inversed pulse-signal $/PLS$. An output of the AND-gate 132 generates

a charge-time control signal. The charge-time control signal determines the length of an on-time t_{CHG} of the switch 133.

[0059] When the pulse-signal **PLS** supplied by the pulse signal generator 200 goes low, the AND-gate 132 will output the charge-time control signal in response to the magnitude of the first multiplier-signal V_E .

[0060] The charge-time control signal is supplied to the linear charging block. The linear charging block includes a capacitor 135 and two switches 133 and 134. An input terminal of the switch 133 is supplied with the constant current I_R . An output of the switch 133 is connected to an input terminal of the switch 134. A control terminal of the switch 133 is connected to an output of the AND-gate 132. An output terminal of the switch 134 is connected to the ground reference. A control terminal of the switch 134 is supplied with the clear-signal **CLR**. The capacitor 135 is connected in parallel with the switch 134. The on-time t_{CHG} of the switch 133 will be proportional to the first multiplier-signal V_E and will be inversely proportional to the magnitude of the divisor-signal V_{AC} .

[0061] When the switch 133 is closed by the charge-time control signal supplied by the AND-gate 132, the capacitor 135 will begin to be charge by the constant current I_R . When the pulse generator 200 generates a clear-signal **CLR**, the switch 134 will close, and the charge stored in the capacitor 135 will be discharged.

[0062] The capacitor 135 generates a charge signal V_{CHG1} , which is supplied to the sample-and-hold circuit. The sample-and-hold circuit includes an OPA 136, a switch 137, and a capacitor 138. A positive input of the OPA 136 is connected to the output terminal of the switch 133. A negative input of the OPA 136 is connected to an output terminal of the OPA 136. An input terminal of the switch 137 is connected to the output

terminal of the OPA 136. A control terminal of the switch 137 is supplied with the sample-signal **SMP** of the pulse generator 200. The capacitor 138, which is connected between an output terminal of the switch 137 and the ground reference, generates an output signal V_1 .

[0063] The OPA 136 is a buffer for the charge of the capacitor 135. When a logic-high sample-signal **SMP** from the pulse generator 200 closes the switch 137, the voltage at the output terminal of the OPA 136 will be equal to the potential of the capacitor 135. The maximum voltage of the capacitor 135 will determine the output signal V_1 of the first multiplier-divider stage 130. The magnitude of the output signal V_1 will be proportional to the magnitude of the first multiplier-signal V_E multiplied by the magnitude of the constant current I_R , divided by the magnitude of the divisor-signal V_{AC} . The capacitor 138 is included as a holding capacitor.

[0064] The output signal V_1 of the first multiplier-divider stage 130 of the multiplier-divider 100 is coupled to the second multiplier-divider stage 150 of the multiplier-divider 100. The second multiplier-divider stage 150 of the multiplier-divider 100 also has a charge-time control circuit, a linear charging block, and a sample-and-hold circuit with the same components as the first multiplier-divider stage 130.

[0065] The first multiplier-divider stage 130 of the switched-charge multiplier-divider 100 is implemented according to the principles of capacitor charge theory. An important equation describing the behavior of capacitors is:

$$Q = C \times V = I \times T \text{ ----- (3)}$$

where Q is the charge stored in the capacitor, C is the capacitance of the capacitor, V is the voltage across the capacitor, I is the charge current, and T is the charge time.

[0066] According to equation (3), the voltage across the capacitor C_{135} can be expressed as:

$$V_{CHG1} = \frac{I_R \times t_{CHG}}{C_{135}} \text{-----} (4)$$

where the constant current I_R is used to charge the capacitor 135.

t_{CHG} refers to the length of time that the charge current I_R is applied to the capacitor 135. This can be expressed as:

$$t_{CHG} = \frac{\Delta t \times V_E}{V_{AC}} \text{-----} (5)$$

[0067] Here, V_E is the first multiplier-signal of the first multiplier-divider stage 130 of the multiplier-divider 100. V_{AC} is input into the sawtooth signal generator 110. Δt is the off-period of the pulse-signal PLS generated by the pulse generator 200. The off-period Δt of the pulse signal PLS is constant for the purposes of this operation (see FIG. 9). Thus, equation (4) can be rewritten as:

$$V_{CHG1} = \frac{I_R}{C_{135}} \times \frac{V_E}{V_{AC}} \times \Delta t \text{-----} (6)$$

[0068] Since I_R , C_{135} , and Δt are constants, equation (6) can be simplified to:

$$V_{CHG1} \propto \frac{V_E}{V_{AC}} \text{-----} (7)$$

[0069] After the charging of the capacitor 135 is completed, the sample-and-hold circuit of the first multiplier-divider stage 130 will buffer the charge signal V_{CHG1} . The magnitude of the output signal V_1 of the first multiplier-divider stage 130 will be equal to V_{CHG1} .

[0070] Thus, the basic principles of the first multiplier-divider stage 130 of the multiplier-divider 100 according to the present invention are described above. The

second multiplier-divider stage **150** of the multiplier-divider **100** is built according to the same principles as the first multiplier-divider stage **130**.

[0071] Thus, according the equation (6), the output V_O of the second multiplier-divider stage **150** can be expressed as:

$$V_O = \frac{I_{AC}}{C_{155}} \times \frac{V_1}{V_{AC}} \times \Delta t \text{-----} (8)$$

C_{155} and Δt are constants. Combining equation (7) and (8), the output signal V_O of the multiplier-divider **100** can be expressed as:

$$V_O \propto \frac{I_{AC} \times V_E}{V_{AC}^2} \text{-----} (9)$$

[0072] FIG. 8 shows the second multiplier-divider stage **150** according to a preferred embodiment of the present invention. The second multiplier-divider stage **150** includes a comparator **151**, an AND-gate **152**, three switches **153**, **154** and **157**, two capacitors **155** and **158**, and an op amplifier (OPA) **156**. A positive input of the comparator **151** is supplied with the output signal V_1 of the first multiplier-divider stage **130**. A negative input of the comparator **151** is supplied with the sawtooth signal V_{SAW} . A first input of the AND-gate **152** is connected to an output of the comparator **151**. A second input of the AND-gate **152** is supplied with the inversed pulse-signal /PLS of the pulse generator **200**. A control terminal of the switch **153** is driven by an output of the AND-gate **152**. An input terminal of the switch **153** is connected to the second multiplier-input terminal **IAC**. An output terminal of the switch **153** is connected to an input terminal of the switch **154**. An output terminal of the switch **154** is connected to the ground reference. The capacitor **155** is connected in parallel with the switch **154**. A positive input of the OPA **156** is connected to the output terminal of the switch **153**. A negative input of the OPA **156** is connected to an output of the OPA **156**. The switch

157 is connected between an output terminal of the OPA 156 and the output terminal OUT of the multiplier-divider 100. The capacitor 158 is connected between the output terminal OUT of the multiplier-divider 100 and the ground reference.

[0073] FIG. 9 is a timing diagram illustrating the operation of the pulse generator 200. The pulse generator 200 supplies the pulse-signal PLS, and the inversed pulse-signal /PLS, the sample-signal SMP, and the clear-signal CLR. The sample-signal SMP follows the pulse-signal PLS after a delay time t_{D1} . The clear-signal CLR follows the sample-signal SMP after a delay time t_{D2} .

[0074] When the pulse generator 200 generates the pulse-signal PLS, the sawtooth signal generator 110 will create the sawtooth signal V_{SAW} in response to the divisor-signal V_{AC} . After the pulse-signal PLS goes low, the charge-time control circuit will compare the sawtooth signal V_{SAW} with the first multiplier-signal V_E to produce the on-time of the switch 133. The length of the on-time t_{CHG} will be proportional to the magnitude of the first multiplier-signal V_E divided by the magnitude of the divisor-signal V_{AC} . The linear charging block will charge the capacitor 135 for the duration of the on-time t_{CHG} . The constant current I_R will charge the capacitor 135. At this point, the charge of the capacitor 135 will determine the magnitude of the output signal V_1 of the first multiplier-divider stage 130 of the multiplier-divider 100. When the pulse generator 200 supplies a logic-high sample-signal SMP, the sample-and-hold circuit will hold the output signal V_O of the multiplier-divider 100 across the capacitor 158. The pulse generator 200 will generate the clear-signal CLR following the sample signal SMP, to reset the multiplier-divider 100.

[0075] It will be apparent to those skilled in the art that various modifications and variations can be made to the structure of the present invention without departing

from the scope or spirit of the invention. In view of the foregoing, it is intended that the present invention cover modifications and variations of this invention provided they fall within the scope of the following claims or their equivalents.